Joint Maximum Likelihood Approach to Frame Synchronization in Presence of Frequency Offset

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SUMMARY This paper proposes new frame synchronizers that can achieve frame sync in the presence of a frequency offset. In particular, a maximum likelihood (ML) algorithm for joint frame synchronization and frequency estimation is developed for additive white Gaussian noise (AWGN) channels, then the result is extended to frequency selective channels. Computer simulations demonstrate that the proposed schemes can outperform existing methods when a frequency offset exists.

key words: frame synchronization, maximum likelihood, frequency offset

1. Introduction

For efficient digital communications using burst transmission, reliable frame synchronization that realizes the start of known symbols in a data frame at the receiver is essential. Popular frame synchronization techniques include the correlation rule, which correlates the received signal with a sync pattern, and its modifications [1]–[4]. These techniques have been derived for AWGN channels under the assumption of a perfect carrier recovery. However, since frame synchronization is usually performed before the carrier recovery is completed, the performances of the synchronizers in [1]–[4] can be degraded in practical situations where frequency and phase errors exist.

To overcome this difficulty, methods of frame synchronization that are tolerant of frequency and phase errors have been developed in [5]–[8], including ML rules, with the exception of an ad hoc rule in [5], for AWGN [6], [7] and frequency selective channels [8]. The ML rules are derived following two different approaches. The first is the Bayesian approach adopted in [6], [7], which involves averaging a probability density function (pdf) over the transmitted data, frequency, and phase offsets, while the second is the joint estimation approach adopted in [8], which jointly achieves frame sync, plus a frequency, and channel estimation. In this case, for the derivation, the rule assumes a special sync pattern that is periodically repeated.

In this paper, we first present a new ML rule for AWGN channels based on a joint estimation approach. Then, in relation to the problem discussed in [8], an ML rule is derived that allows an arbitrary sync pattern. Finally, the advantage of the proposed rules over existing schemes is demonstrated through computer simulations. In particular, it is shown that the false acquisition probabilities (FAPs) of the proposed method are smaller than those of existing schemes.

The organization of the remainder of this paper is as follows. Section 2 presents the signal model, the proposed joint ML rules are derived in Sect. 3, and the simulation results are presented in Sect. 4.

2. Signal Model

Consider packet transmission over a dispersive channel where the dispersion spans up to L symbol intervals. It is assumed that a packet starts with a data sequence of length P followed by a training sequence consisting of L − 1 guard symbols and a sync pattern of duration Ns (Fig. 1). The guard symbols are inserted to avoid the sync pattern being affected by random data. After the sync pattern, the data symbols are continued. The training sequence is denoted by \{s_{L+1}, ..., s_{-1}, s_0, ..., s_{N_s-1}\}, in which the first L−1 samples represent guard symbols. It is assumed that the symbols are transmitted in an M-ary PSK format. The received baseband signal, which is sampled with a symbol interval T_s, is expressed as

$$r_k = \sum_{l=0}^{L-1} h_l e^{j\theta_{k-l} + j2\pi f h_{l,k}} + w_k$$  

where \(e^{j\theta_k}\) is the M-ary phase-modulated symbol at time \(k\); \(L−1\) represents the channel memory; \(h = [h_0, h_1, ..., h_{L-1}]^T\)

![Fig. 1 Frame structure.](image)
is a vector containing $T_s$-spaced samples of the channel response; and $f_0$ denotes the frequency offset. Complex AWGN is denoted by $w_k$, and its variance $\sigma_w^2 = N_0/E_s$ where $E_s$ represents the symbol energy and $N_0$ is the noise power. For the AWGN channels, $L = 1$ and $h_0 = e^{j\phi_0}$ where $\phi_0$ is the phase offset. In this case, $r_k$ in (1) is reduced to

$$r_k = e^{j(\theta_k + 2\pi f_0 T_s k + \phi_0)} + w_k. \quad (2)$$

Throughout this paper, frame synchronization is started under the assumption that the position of a packet is roughly known up to an uncertainty of $\mu \in \{0, 1, \ldots, P + L - 1\}$ symbols (such coarse frame sync can be achieved by automatic gain control [8]). A frame is synchronized using $N$ received samples $\{r_0, r_1, \ldots, r_{N-1}\}$. The observation window size $N \geq N_s + P + L - 1$, otherwise some received samples corresponding to the sync pattern may be excluded.

### 3. Derivation of Proposed Frame Synchronization

#### 3.1 Frame Synchronization in AWGN Channels

Figure 2 illustrates the received sequence $r = \{r_0, r_1, \ldots, r_{N-1}\}$ in the observation window and corresponding transmitted sequence for an AWGN channel. If the sync pattern starts at the $\mu$-th position, $\mu \in \{0, P\}$, then the conditional pdf $p(r \mid \mu, f_0, \phi_0)$ is given by

$$p(r \mid \mu, f_0, \phi_0) = \frac{1}{M^{N-N_s}} \sum_{\mathbf{d} \in \mathbb{D}} p(r \mid \mu, f_0, \phi_0, \mathbf{d}). \quad (4)$$

To simplify this expression, the information symbol $e^{j\phi_0}$ is approximated as $e^{j\alpha}$, where $\alpha$ has a uniform distribution over $(-\pi, \pi)$ [1, p.283]. Then

$$p(r \mid \mu, f_0, \phi_0) \approx \left(\frac{E_s}{\pi N_0}\right)^N \prod_{k=\mu}^{\mu+N_s-1} e^{-\frac{\|r_k - e^{j\theta_k} e^{j(2\pi f_0 T_s k + \phi_0)}\|^2 E_s}{2 N_0}}. \quad (5)$$

where $\Omega = \{\mu, \mu + 1, \ldots, \mu + N_s - 1\}$ and $I_0(x) = \frac{1}{\pi} \int_0^\infty e^{-x \cos \theta} d\theta$ is a zeroth-order modified Bessel function of the first kind. The conditional pdf in (5) is further simplified by approximating $I_0(x)$ as $e^{|x|}/\sqrt{\pi}$ [4]:

$$p(r \mid \mu, f_0, \phi_0) \approx C(r) \cdot \prod_{k=\mu}^{\mu+N_s-1} e^{-\frac{|r_k|^2}{2 N_0}} \cdot \prod_{k=\mu}^{\mu+N_s-1} e^{\frac{2N_0}{N_0} |r_k|^2} \cdot \prod_{k=\mu}^{\mu+N_s-1} |r_k|^2 \cdot |r_k|^2 \cdot |r_k|^2 \cdot |r_k|^2. \quad (6)$$

where $C(r) = \left(\frac{E_s}{\pi N_0}\right)^N \prod_{k=0}^{N_s-1} e^{-\frac{|r_k|^2}{N_0}}$. After taking the logarithm, dropping the terms independent of $\mu, f_0$, and $\phi_0$ and subtracting a constant $\sum_{k=0}^{N_s-1} |r_k|^2$, the following test function is obtained:

$$\Lambda(\mu, f_0, \phi_0) \equiv \sum_{k=\mu}^{\mu+N_s-1} \text{Re}[r_k s_k^* e^{-j(2\pi f_0 T_s k + \phi_0)}] \cdot \sum_{k=\mu}^{\mu+N_s-1} |r_k|^2 \cdot |r_k|^2 \cdot |r_k|^2 \cdot |r_k|^2 \cdot |r_k|^2 \cdot |r_k|^2. \quad (7)$$

where $l = k - \mu$ and $\phi'_0 = \phi_0 + 2\pi f_0 T_s \mu$. When the frequency and phase offsets are zero, this expression reduces to the ML rule for a high SNR derived in [2]. The maximization of $\Lambda(\mu, f_0, \phi'_0)$ with respect to $\mu, f_0$, and $\phi'_0$ can be achieved through the following three-step procedure [1, p.248]:

First, maximize $\Lambda(\mu, f_0, \phi'_0)$ with respect to $\phi'_0$ for each possible $\mu$ and $f_0$. Specifically, an estimate of $\phi'_0(\mu)$ is obtained as a function of $\mu$ and $f_0$: $\phi'_0(\mu, f_0) = \arg \max \Lambda(\mu, f_0, \phi'_0)$.

Second, derive an estimate of $f_0$ as a function of $\mu$, which is expressed as $\hat{f}_0(\mu) = \arg \max \Lambda(\mu, f_0, \phi'_0) = \phi'_0(\mu, f_0(\mu))$.

Third, select $\mu$ with the largest likelihood $\hat{\mu} = \arg \max \Lambda(\mu, f_0, \phi'_0) = \phi'_0(\mu, f_0(\mu))$. To derive $\phi'_0(\mu, f_0)$, $\Lambda(\mu, f_0, \phi'_0)$ is differentiated with respect to $\phi'_0$ and the result is set to zero. This yields

$$\phi'_0(\mu, f_0) = \arg \left\{ \sum_{l=0}^{N_s-1} r_{l+\mu} s_l^* e^{-j2\pi f_0 T_s l} \right\}. \quad (8)$$

\(^1\)Since $\mu$, $f_0$, and $\phi'_0$ are finite, the maximum of $\Lambda(\mu, f_0, \phi'_0)$ can also be found through an exhaustive search [9].
Using (8) in (7) gives
\[
\Lambda(\mu, f_0, \phi_0) = \hat{\phi}_0(\mu, f_0)\end{align}
where \(\Lambda(\mu, f_0) = \left| \sum_{i=0}^{N_s-1} s_i e^{-j2\pi f_i T_s} \right|^2 \). Now \(\hat{f}_0(\mu)\) can be obtained by maximizing \(\Lambda(\mu, f_0)\). Differentiating the square of \(\Lambda(\mu, f_0)\) with respect to \(f_0\) and setting the result equal to zero yields
\[
\sum_{i=1}^{N_s-1} \sum_{m=1}^{N_s-1} (l-m)r_{\mu} s_l^* s_m e^{-j2\pi f_0 T_s (l-m)} = 0. \tag{10}
\]
Then, following the procedure for deriving the frequency estimator in [11],
\[
\hat{f}_0(\mu) = \frac{1}{\pi T_s (R + 1)} \arg \left\{ \sum_{l=1}^{R} \rho_\mu(l) \right\} \tag{11}
\]
where
\[
\rho_\mu(l) = \frac{1}{N_s - 1} \sum_{m=1}^{N_s-1} r_{\mu} s_l^* s_{m+l} s_{m-l}. \tag{12}
\]
When \(\mu\) is known, this estimator is identical to the one in [11]. The design parameter \(R\) enables the adjustment of the acquisition range of the frequency estimate, which is given by \(|\hat{f}_0(\mu)| < \frac{1}{(R+1)T_s}\). The proposed frame synchronization rule is then obtained from (9) and (11):
\[
\hat{\mu} = \arg \max \mu \left\{ \sum_{l=0}^{N_s-1} r_{\mu} s_l^* e^{-j2\pi f_0(\mu)T_s l} - \sum_{l=0}^{N_s-1} |r_{\mu} s_l| \right\}. \tag{13}
\]
where \(\hat{f}_0(\mu)\) is given by (11). When \(\hat{f}_0(\mu) = 0\) and the phase offset \(\phi_0 = 0\), this rule reduces to
\[
\hat{\mu} = \arg \max \mu \left\{ \sum_{l=0}^{N_s-1} r_{\mu} s_l^* s_l^* s_{l-1} - \sum_{l=0}^{N_s-1} |r_{\mu} s_l| \right\}. \tag{14}
\]
The ML rule in (14) is identical to the ML rule in [2], developed for AWGN channels without any frequency and phase offset. The proposed rule in (13) compensates for the frequency offset of \(r_{\mu}\) and then evaluates the correlation with the sync pattern \(s_{\mu}\).

### 3.2 Extension to Frequency Selective Channels

For frequency selective channels, following the approach in [8], a subwindow of length \(N_s\) observing \(r_{\mu} = [r_{\mu}, r_{\mu+1}, \ldots, r_{\mu+N_s-1}]^T\) for each \(\mu \in \{0, 1, \ldots, P + L - 1\}\) is employed and the conditional pdf of \(r_{\mu}\) is derived. Under the assumption that \(\mu\) is the correct sync pattern start position, \(r_{\mu}\) only corresponds to the training sequence (Fig. 3), thus its conditional pdf does not depend on the random data within the packet. This fact greatly simplifies the derivation, because averaging the conditional pdf over all possible data sequences becomes unnecessary. The synchronizer derived below detects the sync pattern start position of the 1st path of a multipath fading channel.

The received vector \(r_{\mu}\) can be written in matrix form [9] as
\[
r_{\mu} = \Gamma(f_0) A h + w_{\mu}\tag{15}
\]
where \(\Gamma(f_0)\) is a diagonal matrix given by
\[
\Gamma(f_0) = \text{diag}[1, e^{j2\pi f_0}, e^{j2\pi f_0}, \ldots, e^{j2\pi(N_s-1)f_0}]\tag{16}
\]
\(A\) is an \(N_s \times L\) matrix with entries
\[
[A]_{i,j} = s_{i-j}, 0 \leq i \leq N_s - 1, 0 \leq j \leq L - 1,\tag{17}
\]
and \(w_{\mu} = [w_{\mu}, w_{\mu+1}, \ldots, w_{\mu+N_s-1}]^T\) is a zero-mean Gaussian vector with the covariance matrix \(N_s / E_s I_{N_s}\). Here \(I_{N_s}\) is the \(N_s \times N_s\) identity matrix. For a given pair \((\mu, f_0, h)\), the vector \(r_{\mu}\) is Gaussian with the mean \(\Gamma(f_0) A h\) and covariance matrix \(N_s / E_s I_{N_s}\). Thus the conditional pdf of \(r_{\mu}\) assuming \(\mu, f_0, h\), and \(h\) takes the form
\[
\rho(r_{\mu} | \mu, f_0, h) = \left( \frac{E_s}{\pi N_s} \right)^{N_s} \cdot \exp \left\{ -(r_{\mu} - \Gamma(f_0) A h)^H (r_{\mu} - \Gamma(f_0) A h) \left( \frac{E_s}{N_s} \right) \right\}. \tag{18}
\]
After taking the logarithm and dropping the terms independent of \(\mu, f_0, h\), this yields
\[
\Lambda(\mu, f_0, h) = -(r_{\mu} - \Gamma(f_0) A h)^H (r_{\mu} - \Gamma(f_0) A h). \tag{19}
\]
To maximize \(\Lambda(\mu, f_0, h)\) with respect to \(\mu, f_0, h\), the three-step approach introduced in the previous section is applied. First a channel estimate is found by setting the derivative of (19) equal to zero. The result is:
\[
\hat{h}(\mu, f_0) = (A^H A)^{-1} A^H \Gamma(f_0) A^H r_{\mu}. \tag{20}
\]
When \(\mu\) and \(f_0\) are known, (20) reduces to the ML channel estimate in [12]. Substituting \(\hat{h}(\mu, f_0)\) in (20) for \(h\) in (19),
\[
\Lambda(\mu, f_0, h) = \hat{\mu}(\mu, f_0)) = r_{\mu}^H \Gamma(f_0) B \Gamma(f_0)^H r_{\mu} - r_{\mu}^H r_{\mu} \tag{21}
\]
\[
= 2 \text{Re} \left\{ \sum_{l=0}^{N_s-1} \rho_\mu(l)r_{\mu} e^{-j2\pi f_0 T_s l} \right\} - \rho_\mu(0) - \sum_{l=0}^{N_s-1} |r_{\mu} l|^2 \tag{21}
\]
where \( B = A(A^H A)^{-1} A^H \),
\[
\rho_\mu(l) = \sum_{m=1}^{N_L-1} [B]_{l-m,m} r_{m+l}^* r_{m-l-\mu},
\]
and \([B]_{i,j}\) is the \((i, j)\)th-entry for \( B \). After dropping the terms independent of \( f_0 \) from (21), the ML frequency estimate can be expressed as
\[
\hat{f}_0(\mu) = \arg \max_{f_0} \left[ 2 \text{Re} \left\{ \sum_{l=0}^{N_L-1} \rho_\mu(l)e^{-j2\pi f_0 T_s l} \right\} - \rho_\mu(0) \right]. \tag{23}
\]

For a given \( \mu \), (23) is the same as the frequency estimator in [9]. This estimate is obtained by exhaustively searching the range \([f_0] \leq 0.5\). Using (23) in (21), the proposed frame sync rule for frequency selective channels is obtained:
\[
\hat{\mu} = \arg \max_{\mu} \left\{ r_{\mu}^H \Gamma(\hat{f}_0(\mu)) A A^H \Gamma(\hat{f}_0(\mu))^H r_{\mu} - r_{\mu}^H r_{\mu} \right\}. \tag{24}
\]

This rule is identical to the one in [8], with the exception that the frequency estimator in (23) is employed (in [8], the frequency offset is estimated assuming a periodic sync pattern with period \( L \)). Due to (23), the proposed rule can employ an arbitrary sync pattern. If the sync pattern is chosen to satisfy \( A^H A = N_L I \), then the rule in (24) becomes
\[
\hat{\mu} = \arg \max_{\mu} \left\{ \frac{1}{N_L} r_{\mu}^H \Gamma(\hat{f}_0(\mu)) AA^H \Gamma(\hat{f}_0(\mu))^H r_{\mu} - r_{\mu}^H r_{\mu} \right\}
\[
= \arg \max_{\mu} \left\{ \frac{1}{N_L} \sum_{i=1}^{L-1} \sum_{k=0}^{N_L-1} r_{k+i}^* s_{k-l} e^{-j2\pi \hat{f}_0(\mu) T_s k}^2 \right\} - \sum_{k=0}^{N_L-1} |r_{k+i}|^2. \tag{25}
\]

The computational load for evaluating (26) is close to that for (24), because matrix \( B \) can be precalculated. Equation (26) is mainly useful for grasping some intuition about the behavior of the proposed scheme. In particular, when the channel is flat fading \((L = 1)\), the rule in (26) becomes almost identical to the one in (13): the only difference is that the former evaluates “squares,” while the latter computes “absolute” values. For frequency selective channels, the proposed rule detects the sync pattern start position of the 1st path by combining the correlations of all paths. Although the rules in (24) and (26) do not require explicit channel estimation, a frequency estimation is needed for each \( \mu \). Since (23) requires an exhaustive search, the major computational burden of the proposed rule comes from the frequency estimation. The frequency offset and channel estimates are given by \( \hat{f}_0(\hat{\mu}) \) and \( \hat{h}(\hat{\mu}, \hat{f}_0(\hat{\mu})) \), respectively, and can be obtained after finding \( \hat{\mu} \).

Finally, in this section, it is worthwhile to derive the rule in [8] from (24). Suppose that the sync pattern is given by a repeated CAZAC (constant-amplitude, zero autocorrelation) sequence [5] with period \( L \). Then \( A^H A = N_L I \), and due to the repetition of a CAZAC sequence, \( B \) becomes
\[
B = \frac{1}{P} \begin{bmatrix} I_L & I_L & \cdots & I_L \\ I_L & I_L & \cdots & I_L \\ \vdots & \vdots & \ddots & \vdots \\ I_L & I_L & \cdots & I_L \end{bmatrix} \tag{27}
\]
where \( P \) is the number of repetitions in the sync pattern \((P = \frac{N_L}{L})\). For the matrix \( B \) in (27), the rule in (24) is simplified to
\[
\hat{\mu} = \arg \max_{\mu} \left\{ -\rho_\mu(0) \left( 1 - \frac{1}{P} \right) + 2 \sum_{m=1}^{P-1} |\rho_\mu(mL)| \cdot \cos \left[ \arg[\rho_\mu(mL)] - 2\pi m \hat{f}_0(\mu) T_s l \right] \right\}. \tag{28}
\]

where
\[
\rho_\mu(l) = \left\{ \begin{array}{cl} \frac{1}{N_L} \sum_{m=1}^{N_L-1} r_{m+lp}^* r_{m-l-\mu} & \text{where } l = 0, L, \ldots, (P-1)L \\ 0, & \text{otherwise.} \end{array} \right. \tag{29}
\]

In [8], (28) is used in conjunction with the following frequency estimate: \( f_0(\mu) = \frac{1}{L T_s} \arg[\rho_\mu(L)] \) for \( \rho_\mu(l) \) defined in (29). The rule in (28) can be thought of as a special case of the rule in (26). Both of them are derived from (24), assuming \( A^H A = N_L I \), but the latter allows an arbitrary sync pattern. However, these rules also exhibit a notable difference. The rule in (26) is based on the correlation between the received signal and the sync pattern. In (28), such a correlation is not obtained; instead, the rule searches for a periodic pattern of duration \( L \) in a received signal by examining the similarity between the received samples \( r_k \) and \( r_{k-L} \) (see (29)). Consequently, the test function in (28) decays slowly as \( \mu \) moves away from the start position of the sync pattern [13]\(^{11}\), thereby degrading the frame synchronization performance (this problem does not occur in (26)). In the next section, the behavior of the rules in (26) and (28) is examined through computer simulation.

4. Simulation Results

The false acquisition probabilities (FAPs)\(^{11}\) for the proposed rules were investigated by simulations using the following parameters: \( M = 4 \) (QPSK), \( N = 80 \), and \( P = 20 \). A sync pattern of length \( N_s = 16 \) was taken from the midamble of GSM, given by

\(^{11}\)To relieve the difficulty, [13] proposes the use of an aperiodic training sequence in which CAZAC blocks are phase-shifted and concatenated. However, this approach requires a longer training sequence with a length of \((N_s + (L-1))P\), because a guard interval of length \( L - 1 \) is appended at the beginning of each CAZAC sequence.

\(^{11}\)Since the sync pattern starts at the \( \mu \)th position, \( \mu \in \{0, 1, \ldots, P - L + 1\} \), of \( N \) observations, the synchronizer only has two stages: it either acquires or false locks. Therefore, the probability of false acquisition completely characterizes the synchronizer performance.
This pattern satisfies $A^H A = N_s I_L$ when $L < 8$. The frequency selective channel was modeled as:

$$h(t) = \sum_{l=0}^{L-1} h_l \delta(t - lT_s)$$

(31)

where $\{h_l\}$ are independently identically distributed complex Gaussian random variables with a zero mean and variance of $1/L$. The simulations used 500,000 independent frames and the FAP was empirically estimated by counting the number of frame synchronization failures$^\dagger$. For comparison, the conventional correlation rule, the rule in [7] for AWGN channels, and the rule in [8], as defined in (28) for dispersive channels, were also considered. It was observed that all these rules could be directly applied to the frame structure shown in Fig. 1. The rule in [7] is expressed as

$$\hat{\mu} = \arg \max_{\mu} \left\{ \rho_{\mu}(l) - \sum_{m=1}^{N_r-1} |r_{m}^{\mu+1}-r_{m-4}\mu| \right\}$$

(32)

where $\rho_{\mu}(l)$ is given by (12). Repeated CAZAC sequences of $\{1, -j, 1, j\}$ ($L = 4$) and $\{1, 1\}$ ($L = 2$) were employed in implementing the rule in (28), while all the other rules in the simulation used the training sequence in (30).

Figures 4 and 5 compare the performances of the rules when $f_0 T_s$ was uniformly distributed over $[-f_m T_s, f_m T_s]$, where $f_m T_s = 0.01$ and 0.1. As expected, the correlation rule generally performed worst, whereas the proposed rule outperformed the others.

The robustness of the frame synchronizers was examined by estimating the FAPs for various normalized frequency offsets ($f_0 T_s$) between 0 and 0.3, while fixing $E_b/N_0$.
Fig. 8 Probability of false acquisition for frequency selective channels of length $L$. The normalized frequency offset was generated randomly over $[-0.10, 0.10]$.

Fig. 9 Probability of false acquisition for frequency selective channels of length $L$. $E_b/N_0$ was fixed at 24 dB.

at 3 dB. The results are shown in Fig. 6. Again, the correlation rule performed worst. The FAP of the proposed rule decreased as $R$ increased, at the expense of a narrower frequency acquisition range. The rule in [7] was most robust to frequency offsets, yet its FAPs were larger than those of the proposed rule when $R = 4$ and 8.

Figures 7 and 8 show the FAPs for the frequency selective channels with $L = 2$ and $L = 4$. As in the case of the AWGN channels, the correlation rule performed worst, and the proposed rule outperformed the others. The performance degradation of the rule in [8] was due to the slow decaying characteristic of the test function, as explained at the end of Sect. 3.

Finally, Fig. 9 compares the robustness of the frame synchronizers to frequency offset in dispersive channels. Both the proposed rule and the rule in [8] were robust to a frequency offset: the robustness of the former resulted from the fact that the acquisition range of the frequency estimator in (23) is given by $|f_0| \leq 0.5$. For all values of frequency offset, the proposed rule performed the best.

5. Conclusion

ML-type frame synchronizers that can jointly achieve frame sync, plus a frequency and channel estimation were derived and the advantages of the proposed techniques over existing ones demonstrated through computer simulation. Further work in this area will include the development of frame synchronizers for systems with transmitter and receiver antenna diversity.

References

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